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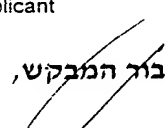
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מערכת אקטיבית להפחתת רעש

(בעברית)
(Hebrew)

ACTIVE ACOUSTIC NOISE REDUCTION SYSTEM

(באנגלית)
(English)

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ACTIVE ACOUSTIC NOISE REDUCTION SYSTEM

מערכת אקטיבית להפחתת רעש

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P-1301-IL

FIELD OF THE INVENTION

The present invention relates generally to noise reduction systems and more particularly relates to acoustic noise reduction systems adapted to reduce the noise at a point relatively far from the noise source.

5

BACKGROUND OF THE INVENTION

Digital adaptive reduction of noise in the time domain is typically performed by sampling the analog output of a microphone that is appropriately positioned to sense the input noise. The sampled analog noise is then converted to digital format via an A/D converter, passed through an adaptive digital filter and then converted back to analog via a D/A
10 converter before being output to a speaker. The analog output of a microphone is utilized as the input to the internal adaptive algorithm within the prior art noise reduction system.

Since the group delay of such a system as described above is relatively large, a typical method of noise reduction employed in the prior art using such a system is to reduce the effect of periodic noise sources as opposed to arbitrary noise sources.

15 Typical prior art noise reduction systems utilize an adaptive digital filter in the main data path to reduce the effect of the noise source. This causes the group delay of the system to be relatively large.

For example, U.S. Patent No. 5,553,154, issued to Tamamura et al., discloses an adaptive filter that receives pulses that are synchronized with the period of the noise. The
20 interval of the input noise determines the length of the taps in the delay line of the adaptive filter.

U.S. Patent No. 5,613,009, issued to Miyazaki et al., discloses a vibration control system that a reference signal from the vibration source and an error signal from an object are input to the adaptive filter. Feedback means generates a feedback control signal in
25 combination with a feedforward signal, forms a drive signal for a vibrating means.

U.S. Patent No. 5,627,896, issued to Southward et al., discloses an active system for controlling noise. The system operates by limiting the output gain from a gradient descent algorithm.

Frequency domain analysis of the input data in the main data path of the system is
30 another common technique utilized by prior art noise reduction systems. For example, U.S.

Patent No. 5,271,062, issued to Sugita et al., discloses a noise reduction system that generates a signal having the same frequency but inverted phase relative to the input noise.

U.S. Patent No. 5,347,586, issued to Hill et al., discloses a noise control system comprising a reference microphone for generating a reference signal that is correlated with
5 the noise emanating a noise source, a plurality of loudspeakers, a plurality of error microphones for generating a plurality of error signals and an adaptive controller.

U.S. Patent No. 5,365,594, issued to Ross et al., discloses a vibration control system that utilizes a vibration input signal derived from a sensor sampling the vibrations to generate an output representative of the interference free vibration of a primary source.

10 U.S. Patent No. 5,519,637, issued to Mthur et al., discloses an active structural acoustic control method for reducing the sound emitted through a structure. The method uses an array of transducers placed in a far field structure and an array of actuators mounted or embedded in that structure. Each is controlled by the system controller and uses reference signals derived from the noise source.

15 Alternatively, another method of noise cancellation used in prior art systems places the microphone as close to the noise source as possible and the loudspeaker relatively far from the microphone so as to create a delay equal to the time for the noise to travel from the microphone to the speaker. This delay is intentionally created in order to match the internal signal processing time of the noise reduction system. The propagation time for the noise is
20 configured to roughly match and compensate for the signal propagation time within the noise reduction system. This noise reduction method is particularly useful for cancellation of noise in a duct such as an air conditioning duct. The internal signal processing is performed during the time that it takes for the sound waves to travel from the microphone to the loudspeaker.

Another prior art noise reduction technique related to the one just described, is to
25 place the speaker close the noise source rather than far away from it, place a second microphone in the desired quiet zone and to adapt a digital filter utilizing the second microphone output. However, this method is useful for canceling repetitive noise only.

The implementation and calibration of noise reduction systems made according to the prior art techniques described above are typically very difficult and correspondingly costly
30 due to the need to supply a plurality of different elements, e.g., two microphones and a loudspeaker, and place these plurality of elements in their appropriate places.

Another disadvantage of prior art noise reduction systems is that if the canceled noise is not periodic in nature, then the physical dimensions of the cancellation system become relatively large. When the loudspeaker is located far away from the noise source, then the noise cancellation is localized and limited to a relatively small area. It would thus be desirable to have a noise reduction system in which the physical design and calibration limitations of prior art noise reduction systems are avoided.

U.S. Patent No. 5,410,607, issued to Mason et al., discloses a noise cancellation system for reducing noise radiated from a complex vibrating surface. The system includes a motion sensor, a controller having fixed transfer function and operative to generate an antinoise signal, and an acoustic driver operative to generate an acoustic antinoise field that is substantially 180 degrees out of phase with the original noise field. The antinoise field reduces the original noise field using destructive interference.

U.S. Patent No. 5,618,010, issued to Pla et al., discloses an active noise reduction system that utilizes a noise radiating panel to generate a noise that cancels the noise source. A piezoceramic actuator is connected to the panel. A sensing device such as an accelerometer is used in generating an opposite noise signal with which to cancel the noise source in the vicinity of the panel.

SUMMARY OF THE INVENTION

The present invention is an active acoustic noise reduction system which comprises an input transducer and an output actuator that are physically located next to each other in the same location. In one embodiment, the input transducer and the output actuator are a hybrid
5 represented by a single element. The active noise reduction system is located as close as possible to the noise source and functions to generate the cancellation sound wave with minimum delay with respect to the noise source.

The active noise reduction system, located very close to the noise source, functions to generate synthetic sound waves having a phase opposite that the noise. In one embodiment of
10 the invention, the noise sound wave and the cancellation sound wave spread almost from the same point producing a high amount of noise cancellation. The output power of the cancellation signal is chosen so as to achieve maximum cancellation of the noise sound.

Another embodiment of the invention is applicable when it is possible to place the noise reduction system very close to the noise source but the noise source body is much larger
15 then the noise cancellation system. In the case when the noise body generates noise having the same phase in a direction towards the noise reduction system, good cancellation is achieved in the far field. Another benefit is that the noise cancellation is based on detecting the noise at only one point on the noise source body.

Another embodiment of the invention is applicable when it is not possible to get close
20 to the noise sound source or when the noise does not emanate from a single point or when the noise source body is relatively large compared to the system. In this case, a plurality of noise reduction systems are placed side by side, i.e., in an array configuration, to produce a 'wall of silence' with each noise reduction system generating cancellation sound waves in accordance with the noise detected at that particular point. Each element of the noise reduction array in
25 this case operate independently of each other as opposed to each element being connected to some central processing unit.

The acoustic cancellation method of the present invention is based on the behavior of acoustic beam patterns in air. Cancellation of the noise is achieved in an area far from the noise source while in an area relatively close to the noise source there may be pockets of
30 noise that exist. The length of the quiet zone, as measured from the noise source, is determined by the power of the cancellation signal generated and output by the system. Since the output acoustic beam pattern is dependent on the characteristics of the output actuator and

on the main cancellation frequency that is used, the type of output actuator or the angle between a plurality of actuators may need to be varied in order to achieve optimum results for different noise frequencies. The noise reduction method of the present invention is capable of achieving effective cancellation of the noise when the surface of the noise source is complex given that the distance from the noise source to the point of cancellation is bigger than the length of the noise source itself.

In addition to sensing sound from the noise source, the system also detects the sound from the output actuator. The portion of the input signal that is due to the output actuator is removed using an echo cancellation technique. If the output and input transducers are acoustically separate elements and there exists acoustic delayed feedback in the system, then using an echo cancellation system is preferred. Another advantage of the echo cancellation system is the elimination of feedback sound emanating from walls, furniture, etc. and sensed by the input transducer. If there is no delayed time feedback from the output transducer to the input transducer and a directional input transducer is used, then a computation may be performed on the input signal, instead of using an echo cancellation system, to discern the actual noise signal from the input signal.

In addition, the cancellation signal generated by the output actuator may be reflected from the noise source itself thus adding to the amount of noise present. In order to eliminate this type of noise, a delayed cancellation signal is generated by the system. The delay and phase shift applied to the cancellation signal is matched to the delay and phase shift associated with the reflection and feedback of the sound from the output actuator.

There is therefore provided in accordance with the present invention an acoustic noise reduction system for reducing the effects of a noise source, comprising input transducer means for sensing the acoustic noise field generated by the noise source and for generating an input signal therefrom, output actuator means for generating an acoustic output field that is effective to reduce the level of the acoustic noise field, correction means for adjusting the input signal generated by the input transducer to compensate for the non linear characteristics of the input transducer and output actuator, echo cancellation means for removing from the input signal a portion of the output of the output actuator means fed back through the input transducer means, the output of the echo cancellation means representing a signal corresponding to substantially the noise source by itself, antinoise means for generating an antinoise signal opposite in phase to the input signal, the output actuator means generating the

acoustic output field from the antinoise signal and wherein the input transducer means is located in relatively close proximity to the output actuator means.

There is also provided in accordance with the present invention an acoustic noise reduction system for reducing the effects of a noise source, comprising input transducer means for sensing the acoustic noise field generated by the noise source and for generating an input signal therefrom, output actuator means for generating an acoustic output field that is effective to reduce the level of the acoustic noise field, correction means for adjusting the input signal generated by the input transducer to compensate for the non linear characteristics of the input transducer, input decoding means for removing extraneous signals from the input signal so as to generate a signal corresponding to substantially the noise source alone, antinoise means for generating an antinoise signal opposite in phase to the input signal, the output actuator means generating the acoustic output field from the antinoise signal and wherein the input transducer means is located in relatively close proximity to the output actuator means.

The correction means comprising storage means for storing a plurality of coefficients, coefficient processing means for dynamically updating the values of the plurality of coefficients stored in the storage means and means for generating a corrected input signal from the contents of the storage means and the input signal.

The correction means comprising storage means for storing a plurality of coefficients, sigma generating means for outputting a signal corresponding to substantially the noise source only, coefficient processing means for dynamically updating the values of the plurality of coefficients stored in the storage means and means for generating a corrected input signal from the contents of the storage means and the input signal.

The echo cancellation means comprises a digital filter having a delay line with a number of taps whose total delay time is equivalent to at least a system time delay of the noise reduction system, adaptation means for dynamically adjusting the coefficient values associated with each of the taps of the digital filter and summing means for adding the output of the digital filter with the output of the correction means.

The antinoise means comprises a variable gain amplifier operative to generate an amplified signal 180 degrees opposite in phase from the input signal and gain control means for dynamically controlling the gain of the variable gain amplifier. The gain control means is adapted to receive a manual input control signal from a user which determines the gain of the

variable gain amplifier, the user able to vary the location of a quiet zone generated by the system by varying the input control signal. The input control signal is generated by the user remotely from the system and transmitted to the system via wireless communication means.

The system further comprises a low pass filter operative to reduce oscillations present in the system derived from feedback of the acoustic output field to the input transducer. Also, the system further comprises delay cancellation means for reducing the effect of echo signals caused by the antinoise means sensed by the input transducer. The delay cancellation means comprises a plurality of delay cancellation circuits wherein each delay cancellation circuit is operative to reduce the effect of the echo caused by previous delay cancellation circuits.

Further, there is provided in accordance with the present invention a method for reducing the effects of a noise source, comprising the steps of sensing the acoustic noise field generated by the noise source and generating an input signal therefrom, generating an acoustic output field that is effective to reduce the level of the acoustic noise field, adjusting the input signal generated by an input transducer to compensate for the non linear characteristics of the input transducer and an output actuator, removing from the input signal a portion of the output of the output actuator fed back through the input transducer, generating a signal corresponding to substantially the noise source by itself and generating an antinoise signal opposite in phase to the input signal, generating the acoustic output field from the antinoise signal.

Also, there is provided in accordance with the present invention a method for reducing the effects of a noise source, comprising the steps of sensing the acoustic noise field generated by the noise source and for generating an input signal therefrom, generating an acoustic output field that is effective to reduce the level of the acoustic noise field, adjusting the input signal generated by an input transducer to compensate for the non linear characteristics of the input transducer, removing extraneous signals from the input signal so as to generate a signal corresponding to substantially the noise source alone and generating an antinoise signal opposite in phase to the input signal, the output actuator means generating the acoustic output field from the antinoise signal.

BRIEF DESCRIPTION OF THE DRAWINGS

The invention is herein described, by way of example only, with reference to the accompanying drawings, wherein:

Fig. 1 is a schematic diagram illustrating the noise reduction system of the present invention applied to an example area having a noise source;

Fig. 2 is a schematic diagram of a single noise reduction system applied to reduce the effect of a noise source showing the acoustic beam patterns generated;

Fig. 3 is a schematic diagram of a plurality of noise reduction systems applied as an array of elements to reduce the effect of a noise source showing the acoustic beam patterns generated;

Fig. 4 is a high level block diagram of a first embodiment of the noise reduction system of the present invention utilizing echo cancellation;

Fig. 5 is a high level flow diagram illustrating the calibration method of the delay cancellation circuit;

Fig. 6 is a high level block diagram illustrating the input transducer and output actuator implemented as a hybrid combination in a single element;

Fig. 7 is a high level flow diagram illustrating the gain control method utilized in the first and second embodiments;

Fig. 8 is a high level flow diagram illustrating the first calibration method associated with the first embodiment;

Fig. 9 is a high level flow diagram illustrating the second calibration method associated with the first embodiment;

Fig. 10 is a high level block diagram of a second embodiment of the noise reduction system of the present invention utilizing a computational method to reduce echoes and oscillations;

Fig. 11 is a high level flow diagram illustrating the first calibration method associated with the second embodiment of the present invention;

Fig. 12 is a high level flow diagram illustrating the echo removal method of the present invention utilized in the second embodiment; and

Fig. 13 is a high level flow diagram illustrating the second calibration method associated with the second embodiment of the present invention.

DETAILED DESCRIPTION OF THE INVENTION

A schematic diagram illustrating the noise reduction system of the present invention applied to an example area having a noise source is shown in Figure 1. The noise reduction system, generally referenced 10, is preferably placed very close to a noise source 24. The distance X is the distance between the noise source and the system 10. The smaller the distance X between the noise source and the system, the better the noise cancellation achieved. The system 10 comprises an input transducer 30 such as a microphone and one or more output actuators such as loudspeakers. In the example system shown in Figure 1, three output actuator loudspeakers 32 are shown. The orientation of the output actuators is such that the sound waves generated by the output actuators cancel the noise source sound waves.

The noise source 24 is shown generating acoustic sound waves 40 that are sensed by the input transducer 30 in system 10. The width of the noise source is denoted by the value W and its length is denoted by the value Y. The system 10 is located from the noise source at a distance X. The width of the system is denoted by the value Z.

The noise source and the system are shown in a typical application such as a living room environment in a residence. The living room area 12 comprises typical furniture found in a living room, for example, two chairs 14, 20, a coffee table 22 and sofa 18. A person 16 is shown seated on the sofa and positioned within the effective quiet zone of the system. Although the noise source 24 and the system 10 are shown as separate entities, an alternative is to place both the system 10 and the noise source within a single enclosure (not shown). If the noise source is placed outside the enclosure, the enclosure is regarded as the noise source. The size of the noise source 24 influences the cancellation of the noise source acoustic waves. If the dimension Y of the noise source is large relative to the wavelength of the shortest interference noise signal, then a second noise reduction system should be installed on the other side of the noise source in order to achieve cancellation on that side.

The mechanical structure of the output actuator used in the system has an effect on the quality of the noise reduction achieved. This is especially true in the case when the width W of the noise source is bigger than the width Z of the system which is related to the length of the output actuators. Preferably, the system 10 is a symmetric structure built from many small output actuator elements wherein each output actuator is oriented in a different direction. The output actuator elements may be spread over the length of the housing enclosing the system in order to provide coverage up to 180 degrees. Note that only one

input transducer 30 (e.g., microphone) is connected to the noise reduction system 10. Each of the output actuators drive the same phase of noise cancellation wave. The number of output actuators can vary in accordance with the particular application and may be reduced to one. Alternatively, the input transducer and the output actuator can be combined in a hybrid input/output element that is positioned against the noise source.

In a case of a hybrid transducer and the use of a plurality of output actuators, only the central actuator is used as a transducer. In the case of both separate input/output transducers and a hybrid transducer, the input transducer 30 must be oriented in a direction towards the noise source 24. The output transducers 32 must be oriented in a direction opposite the noise source. If a plurality of output actuators is utilized, then the centrally located transducer is oriented in a direction opposite the noise source. The output actuators other than the centrally oriented one must be positioned so as to achieve good noise cancellation, especially when a small number of output actuators is used. The proper position for the output actuators can be calibrated either manually or automatically at the time the system 10 is installed. Automatic calibration can be performed utilizing two motors (not shown), each oriented to handle a different axis of motion, attached to the output actuators. The proper calibration angle is determined by using the motors to adjust the position of the actuators to the angle that yields maximum detected power at the input transducer or sensor 30.

The total response time of the system, from the time the noise sound waves reach the input transducer to the time the noise cancellation signal is output by the output actuator, is preferably as short as possible. The effective length X is increased by an amount equivalent to the system delay time for the highest frequency component of the noise source wave.

In general, the system 10 detects the noise source using the input sensor 30, amplifies the noise with inverse polarity and outputs it through the output actuator 32. Since the output actuator and the input transducer are located very close to each other, the contribution of the noise signal to the amplitude of the input signal is much lower than that of the output transducer.

In some configurations the noise cancellation signal generated by the output actuator may be reflected from the noise source as shown by the dashed line 26, thus increasing the overall level of noise in the system. To eliminate this type of reflected noise, a delayed cancellation signal is output by the system.

The acoustic noise cancellation method of the present invention is based on the behavior of the acoustic beam pattern in the air of the noise and the signal output by the system. A schematic diagram of a single noise reduction system applied to reduce the effect of a noise source showing the acoustic beam patterns generated is shown in Figure 2. Good noise cancellation is achieved in an area far both from the noise source and the input transducer/output actuator while in areas close to the noise source there may be zones having higher levels of noise. Note that the system can effectively cancel noise at any arbitrary frequency regardless of whether the noise signal is periodic or not and without requiring any synchronization with the noise source.

The distance Q from the noise source represents an area of relative quiet. The length of Q is determined by the output power of the noise cancellation signal output by the system. Since the acoustic beam pattern is dependent on the characteristics of the output actuators and on the main frequency of the cancellation signal, it may be necessary to use different output actuators or to change the angle between them in order to achieve optimum noise cancellation for noise sources having different frequencies. For noise sources with complex surfaces, it is possible to achieve good noise cancellation when the distance from the noise source to the point of cancellation is larger than the noise source itself.

With reference to Figure 2, a plurality of output actuators 32 is shown generating an anti-noise signal in response to a noise source 50. The sound waves 52 of the anti-noise combine with the original noise waves at a point far from the noise source thus creating a quiet zone. When a plurality of output actuators is used, each of the actuators creates its own anti-noise field oriented at a specific angle. The acoustic field of all of the output actuators acting together combine with the noise source acoustic field to create a high intensity area, a high cancellation area or quiet zone and a low cancellation area. The low cancellation area 52 is due to the effect of noise emitted from points such as 53 that are far from the system. Better noise cancellation is achieved if the noise source body generates homogenous noise, i.e., all of the points 53 generate noise having the same phase. The distance of the quiet zone from the noise source is dependent on the energy content of the anti-noise.

A schematic diagram of a plurality of noise reduction systems applied as an array of elements to reduce the effect of a noise source showing the acoustic beam patterns generated is shown in Figure 3. This scheme is utilized when the surface of the noise source is large and complex or when it is difficult to place the noise reduction system close to the noise

source. Noise cancellation is optimum when the noise generated by the noise source at a particular point on the body of the noise source has the same phase as the noise emitted from other points on the body of the noise that are oriented in the same direction.

Three noise reduction systems 60, 66, 70 are utilized in this example to reduce the effects of the noise source 58. The output actuator 62 of the system 60 functions to generate an anti-noise sound field 64. The output actuator 68 of the system 66 functions to generate an anti-noise sound field 70. Similarly, the output actuator 72 of system 70 functions to generate an anti-noise sound field 76. Thus, an array of independent output actuators 62, 68, 72 is used to create a quiet area at a distance from the array. The effectiveness of the virtual wall of quiet generated by the system is determined by numerous parameters. Such parameters include the distance between the individual noise reduction systems, the mechanical and electrical characteristics of the output actuators in relation to the main noise frequency, and the combined energy generated by the output actuators.

A high level block diagram of a first embodiment of the noise reduction system of the present invention utilizing echo cancellation is shown in Figure 4. The first embodiment, generally referenced 80, of the system comprises means for sensing the noise source, generating an anti-noise signal and outputting this anti-noise signal through one or more output actuators. In addition to sensing the noise source, the input transducer also senses the anti-noise signal output by the output actuator. As described previously, the amplitude of the anti-noise is larger than the amplitude of the noise signal itself. Echo cancellation is utilized to cancel the portion of the input signal associated with the signal output by the output actuator. If the input and output transducers are acoustically separate elements and there exists acoustic delayed feedback in the system, then using an echo cancellation system is preferable. If there is no acoustic delayed feedback from the output actuator to the input transducer, then a computing algorithm may be utilized to extract the noise signal from the total input signal.

The input portion of the system comprises a microphone 84, anti aliasing filter 88, amplifier 90 and A/D converter 92. The microphone is preferably directional and exhibits a very short delay. Use of a directional input transducer directed towards the noise source minimizes the sensitivity to acoustical inputs other than the noise source. Input transducers suitable for use with the present invention include, for example, electromagnetic based transducers, mechanical accelerators, electrical accelerators, piezoelectric and piezoceramic

elements, vibration sensors, a capacitance microphone, a silicon microphone, and an optical microphone.

The analog signal output by the input transducer is then passed through an anti aliasing filter 88 to the analog amplifier 90. The anti aliasing filter 88 is a low pass filter (LPF) having a cutoff frequency of approximately 1 MHz and is constructed to exhibit minimum delay. The fixed gain analog amplifier 90 is adapted to reduce input transducer sensitivity to the minimum needed in order to eliminate the response of the system to sounds originating from sources other than the noise source. The signal output from the fixed gain analog amplifier 90 is then converted to digital via A/D converter 92. The A/D converter is sampled at a rate of approximately 1 M samples/sec and has a resolution of at least 12 bits with 16 bits being preferred.

The digital data output from the A/D converter is then adjusted to compensate for non linearities in the output transducer. Compensation for non linearities include multiplying the digital data by a coefficient stored in a look up table (LUT) 97 via the multiplier 93. The coefficients are calibrated dynamically during operation of the system. A coefficient processor 99 functions to calibrate the LUT coefficients based on the digital data output of the A/D converter and the output of the summer 94.

The output of the multiplier 93 is input to an echo canceler 95 which functions to remove the echo reflected back from the output actuator and picked up by the input transducer. The cancellation signal generate by the echo canceler 95 is added to the output of the multiplier 93 via summer 94. The output of the summer 94 is input to a low pass filter 100 which limits the maximum frequency within the system. LPF 100 is a digital finite impulse response (FIR) filter having a maximum delay of 10 μ s with 3 to 4 μ s preferred. The use of the digital low pass filter 100 having a very short delay is optional but is useful to limit the band pass of the system to help avoid high frequency oscillations caused by the effect of feedback.

The output of the digital low pass filter 100 is input to a variable gain digital amplifier 108 whose gain is controlled by a gain control circuit 106. The variable gain amplifier functions to perform an inversion of the noise signal to generate an anti-noise signal which functions to cancel the effects of the noise. Thus, the gain control circuit 106 sets the gain of the amplifier to a negative gain value. In addition to generating the basic anti-noise signal, the amplifier 108 functions to prevent oscillations from occurring in the system. This is

achieved by controlling the gain of the amplifier 108. The gain of the amplifier can be adjusted relatively slowly and does not have to be performed in real time.

A second input to the gain control circuit 106 is a manual gain control input that is provided by a user. A user can interact with the noise reduction system 10 by adjusting the gain of the amplifier 108. Using a suitable input device such as a remote control, a user positioned such as shown in Figure 1, can control the location of the quiet zone to be any distance from the noise source by adjusting the gain of the amplifier. The gain adjustment capability of the noise reduction system is meant to achieve maximum cancellation at any arbitrary point within the cancellation zone. The gain may be preset or adjusted manually, such as by remote control. The gain control circuit 106 also comprises protection against the gain being increased too high so as to cause oscillations.

The level of gain required to create a suitable quiet zone of high noise sound cancellation is dependent on several factors, e.g., the particular noise source, acoustics and dimensions of the area, the position of the user, etc. For known fixed sources of noise, e.g., air conditioners, vacuum cleaners, etc., the gain adjustment of amplifier 108 can be performed once at the time of installation of the noise reduction system. The gain control method is described in more detail hereinbelow.

The output of the amplifier 108 is input to a summer 112 and a delayed cancellation circuit 110. The output of the delayed cancellation circuit 110 is added to the output of the amplifier 108 via summer 112. The function of the delayed cancellation circuit is to generate a cancellation signal in response to reflections of the output signal from the output actuator (Figure 1 at 26) produced by the noise cancellation system itself. The reflection is effected by the acoustical environment, the distance of the system from the noise source 24 and the frequency of the noise. The delayed cancellation circuit is based on a delay circuit in combination with a negative gain multiplier. In the alternative, the circuit can be based on a digital filter having the same impulse response as the reflected signal but with the opposite, i.e., negative, polarity. The noise reduction system 10 effectively considers the acoustic waves reflected from the noise source as a second mirrored noise source located at a distance equal to the distance between the noise source and the noise reduction system. The only difference being that the path of the acoustic sound waves from the second noise source is in the opposite direction from the sound waves emitted from the noise source itself.

The output of the delayed cancellation circuit is added to the output of the amplifier 108. Note that the signal generated to cancel the first reflection may itself be reflected off the noise source to effectively create a third mirror noise source and so on and so forth. This third noise source can subsequently be canceled using the same method of the delayed cancellation circuit 110 but with different parameters (not shown).

Note that the delayed cancellation circuit is optional but using it, however, can aid in canceling acoustic sound waves fed back from the noise source body. Calibration of the gain and the delay of the impulse response of the delayed cancellation circuit 110 is performed once during installation of the noise reduction system 10. A high level flow diagram illustrating the calibration method of the delay cancellation circuit is shown in Figure 5. The calibration procedure comprises first turning off the noise source and the echo canceler within the system (step 290). Then, a single impulse is generated and output through the output actuator (step 292). The impulse is generated towards the noise source while the noise source itself is off. The impulse response is then measured, i.e., the input fed back from the noise source is measured (step 294). The noise reduction system 10 regards this source of noise as a second noise source having known characteristics.

The measured impulse response is then sampled (step 296) and FIR filter coefficients are generated based on the sampled impulse response (step 298). The gain of the delayed cancellation circuit 110 is determined using the following equation.

$$GAIN_{DCC} = -GAIN_{AMP} \cdot \left(\frac{INPUT}{OUTPUT} \right)$$

Wherein $GAIN_{DCC}$ is the gain of the delay cancellation circuit, $GAIN_{AMP}$ is the gain of the variable gain amplifier 108, INPUT is the maximum amplitude of the response measured at the output of the A/D converter 92 before the data is corrected for non linearities and OUTPUT is the output impulse transmitted value of the variable gain amplifier 108. Thus, the gain of the delayed cancellation circuit (DCC) is based on the negative or inverted gain of the amplifier 108.

Note that the initial portion of the measured impulse response is due to the input transducer picking up the output of the output actuator without echoes, reflections or feedback. The actual response to the impulse function does not begin until a certain time period after the impulse is generated. This time period is proportional to the system time delay period and can be calculated since the start of the impulse function and the measured

response are known. The portion of the impulse response prior to the system delay period is discarded and not used to generate the coefficients for the digital FIR filter that can be utilized in the delayed cancellation circuit. For example, if it is assumed that the system delay time is 10 μ s, then the first 10 μ s of the measured impulse response is discarded. The portion of the response 10 μ s and beyond is sampled and used to generate the filter coefficients. If the system includes cancellation circuitry for the third mirrored noise source, then the calibration is performed in steps. In the first step, the second mirrored source cancellation coefficient calibration is performed as described above. With this cancellation activated, calibration of the second step is performed by repeating the procedure described in Figure 5. The new coefficients are derived from the second feedback filter (not shown).

The output of the digital summer 112 is input to the D/A converter 114 and to the echo canceler 95 portion of the system. The echo canceler 95 comprises a digital filter 96, an adaptation circuit 98 and a summer 94. The echo canceler 95 functions to remove reflections of sound and prevent oscillations caused by the output of the output actuator feeding back to the input transducer. The filter 96 is a digital FIR filter having a sufficient number of taps, i.e., delay, to cover the round trip delay through the system as well as feed back echoes from the acoustical environment. Real time adaptation of the digital filter coefficients by the adaptation circuit 98 is performed using any suitable FIR adaptation algorithm well known in the art, such as the least mean squares technique. The adaptation is based in the error signal output by the summer 94.

The output of the summer 94 is a digital signal wherein the feedback, i.e., echo, caused by the generated output signal has been removed. The digital filter 96 functions to generate a signal that is substantially the opposite of the portion of the input signal that is fed back from the output signal.

The response of the adaptive digital filter 96 is the same response of that of the system from the output actuator to the input transducer including the environmental acoustic effects. The digital filter 96 functions to generate the signal output by the output transducer but with opposite polarity, i.e., negative polarity and the correct phase shift and amplitude. The summer 94 adds the output of the digital filter 96 with the output of the multiplier 93, which is the digital input corrected for the non linearities of the input transducer, to eliminate the echo from the input signal. The addition operation performed by summer 94 may be performed digitally as described above or can be performed in analog. The summing can be

performed in analog by utilizing a D/A converter to convert the output of the digital filter 96 to analog and summing the result with the analog signal from the input transducer. In the case of the analog echo cancellation summation, it is not economical to use an analog multiplier for the linearity table and thus, the assumption is that the actuator is linear. In either case, the output of the echo canceler is input to the digital low pass filter 100 as described hereinabove.

It is important to note that the time response of the digital filter 96 must be long enough to cancel all of the acoustical sound fed back to the input transducer from the output actuator. The adaptive echo canceler 95 adjusts the filter taps in response to changes in the acoustical environment, e.g., temperature, furniture placement, etc.

The output of the summer 112 is input to the D/A converter 114 which functions to convert the digital signal into analog. The output of the D/A converter 114 is input to an analog low pass filter 116. The cutoff frequency of the low pass filter 116 is approximately 1 MHz. The output of the low pass filter 116 is input to the power amplifier 118. The power amplifier boosts the level of the output sufficiently to drive the output actuator 120. The output actuator can be any suitable device that transforms the output signal to sound waves. The output actuator can comprise a loudspeaker having a relatively short delay. The output actuator 120 may comprise a single output actuator or a plurality of output actuators connected in parallel.

In addition, the system of Figure 4 also comprises a controller (not shown) which functions to administer and control the configuration, operation, settings and all timing of the noise reduction system 10.

It is noted that the sound emitted from the output actuator is detected by the input transducer at a much higher amplitude than the noise itself. The noise reduction system 10 functions to discern the much smaller noise signal from the much larger echo signal. However, the input transducer exhibits a non linear response to the amplitude of the sound waves incident on it. It turns out that the input/output response of the input transducer, such as a microphone comprising a membrane, is dependent on the total amount of power hitting the microphone. Thus, for the same amplitude noise signal, the linearity of the microphone is different for an input with low total power input as compared to an input with high total power. Thus, the high amplitude signal output from the output actuator effects a different relative output signal from the input transducer due to the noise. This is especially true when

using a hybrid to perform both the input and the output transducer functions of the system. Non linearity at the output actuator is manifested when the output peak power to the transducer is large. When using separate input/output devices, the non linearity in the output device is much more critical when the mechanical amplitude is large. The operation of the system is based on the correct discrimination of the noise source from the much larger echo signal. Thus, a correction of the echo signal amplitude as it appears in the input is required in order to achieve good cancellation of the echo signal. The linearity LUT performs this correction operation by multiplying each input value with the correction coefficient. The linearity table may be generated a priori and calibrated at the time of installation or adjusted dynamically on the fly. The linearity table and the dynamic adjustment of its contents are described in more detail hereinbelow.

A high level block diagram illustrating the input transducer and output actuator implemented as a hybrid combination in a single element is shown in Figure 6. As an alternative to a separate input transducer and output actuator, a hybrid input/output (I/O) element or transducer 162 can be utilized that performs the functions of both elements. In this case, a hybrid circuit 160 is needed to interface the I/O element 162 to the power amplifier 164 and the anti aliasing filter 166. The hybrid 160 functions to transfer power from the power amplifier 164 with minimum losses to the I/O transducer element 162 and with maximum reduction to the anti aliasing filter 166.

The gain control method implemented in the gain control circuit 106 (Figure 4) of the variable gain amplifier 108 will now be described in more detail. A high level flow diagram illustrating the gain control method utilized in both the first and second embodiments is shown in Figure 7. This method operates in a loop to continuously search for oscillations in the system. In general, an FFT performed in the gain control circuit is used to map the mean amplitude of the frequency content in the detected input. When a new frequency is detected or when the total input power to the system increases, an immediate reduction of the gain of the amplifier 108 is performed.

The first step is to check the total power of the output signal to see if it is over a predetermined maximum (step 130). If the power is over the permitted maximum then the gain is reduced until the total output power is below the maximum (step 132). Once the gain is within the permitted range, the current gain setting is stored as the initial gain value (step 134). A Fast Fourier Transform (FFT) is then performed on the signal input to the amplifier

(step 136). The FFT yields a map of the frequency content of the input signal. A plurality of samples of the input are taken and FFT analysis performed on each sample. Corresponding frequency elements are averaged over many samples (step 138).

It is then checked for the significant presence of signal content at new frequencies (step 140). If signal content is found at new frequencies, these frequencies elements are tracked over time (step 142) to determine whether they are oscillations (step 144). A new frequency that is persistent in time is considered a suspect oscillation. If there is a suspected oscillation, then the gain is reduced by a step amount (step 146). If the gain is reduced to a predetermined minimum (step 148) the frequencies that were suspect as oscillations are mapped as input noise, i.e., a frequency generated by the environment with a particular amplitude and frequency range and not as oscillations (step 152). This is because, at such low values of gain, it would be highly improbable that the suspect frequencies were caused by oscillations. Signals within the frequency range are treated as environmental noise. After the environmental frequencies are mapped, the gain is restored to the gain that was initially saved during step 134.

If there are no new frequency elements in step 140 or oscillations suspected in step 144, the method ends. If the gain in step 148 is not a minimum, than another group of samples is input (step 150). After sampling another group of input signals, it is then checked whether oscillations are still present after the gain has been reduced. The method keeps looping by checking for oscillations, reducing the gain if oscillations are found and generating additional input sample until either no oscillations are found or the gain reaches a minimum.

As described previously, the linearity LUT 97 is used to correct the non linear behavior of the input/output transducers. Since typical input transducers are constructed from moving mechanical parts, the output response for the same input noise level is different for different levels of total input power incident on the input transducer. However the output actuator suffers from non linearities when the motion of the moving mechanical parts increase as a result of increasing output power. The difference in output response of the output actuator and input transducer is corrected utilizing the linearity LUT 97. The linearity LUT stored different coefficients for each amplitude input value range. The linearity LUT is divided into regions with each region having its own coefficient value. For example, assuming a 12 bit data word, the linearity LUT may be divided into 256 regions, thus only

utilizing 8 bits of the input data. Upon startup of the noise reduction system 10, all of the coefficients in the linearity LUT have the same value.

The present invention includes a first and a second method of calibrating the linearity LUT. Both methods are performed in real time during the operation of the noise reduction system. Both calibration methods utilize a linearity look up table (LUT) that holds coefficients used to adjust the input data output by the A/D converter. The adaptation or calibration of the coefficients of the linearity LUT serves to compensate for slow changes to the linearity of the system caused by temperature, etc. The linearity LUT also functions to compensate for the mechanical non linearities of both the input transducer and the output actuator(s). Although not necessary to perform the invention, the input amplitude is divided into a plurality of regions wherein each region has a coefficient associated with it.

The first calibration method utilizes the input noise signal itself to calibrate the coefficients. In the second method, a small amplitude calibration signal is injected into the system during operation and the results used to generate new coefficient. Each calibration method will now be described in more detail below. The high level flow diagrams describing the linearity table calibration methods refer to the calibration of one coefficient. The methods described are repeated in order to calibrate all the coefficients.

A high level flow diagram illustrating the first calibration method associated with the first embodiment is shown in Figure 8. The first method of calibration utilizes the fact that the noise is physical and continuous. The controller in the system tracks the relationship between values termed Table Input (TI), Table Output (TO) and Summer Output (SO) during operation of the system. The TI values are measured at the output of the A/D converter 92 (Figure 4), the TO values are measured at the output of the multiplier 93 and the SO values are measured at the output of the summer 94. The coefficient processor 99 functions to calculate new LUT coefficients based on the TI, TO and SO values.

The calibration of the LUT coefficients during operation of the system attempts to ignore the effects of the noise source. Note that the input noise source itself changes between two adjacent samples. Note also that the output of the summer SO represents the noise source since the echo canceler 95 effectively removes the echo signal from the input signal.

The calibration method initially measures two TO values, i.e., a value at time 'n-1' and another at time 'n'. Subsequently, after a system time delay, the controller then measures the two TI and SO values that are the effect of the previously measured TO values, assuming

the system time delay is known. In other words, each TI and SO value is measured after the corresponding TO values has had a chance to propagate through the system, i.e., output by the output actuator, sensed at the input transducer, etc. Note that the SO value is the TI value after compensation for non linearities and after the echo feedback from the output actuator to the input transducer is removed to yield a value that reflects the noise level only.

With reference to Figure 8, the first step in the calibration method is to read a Table Output (TO) value at the output of the multiplier 93 (Figure 4), termed TO_{n-1} (step 210). After reading the TO_{n-1} value, the system waits for the output of the multiplier to change before reading the next value which is termed TO_n (step 214). During operation of the system, it is not unusual if the input data does not vary much from sample to sample. This is due to the fact that the sampling rate of the system is orders of magnitude higher than the frequencies making up the noise signal. In step 214, the system waits more than one sample time, and the sample is taken when the difference between the level of TO_{n-1} and TO_n reaches some minimum which is predetermined. This minimum determines the coefficient calibration accuracy. It is then determined whether TO_n is within the same region of the LUT as TO_{n-1} (step 216). This is checked in order to prevent two TO values being associated with different regions of the LUT. The calibration method calculates new coefficients for a single region of the LUT at a time. The calculations, thus, cannot span borders between regions.

Next, the system waits for the effect of the TO_{n-1} value (step 218) and TO_n value (step 222) to appear at the output of the A/D converter and the output of the summer. As described previously, the data output by the A/D converter is termed Table Input (TI) data and the data output by the summer is termed Summer Output (SO). Once the effect of the TO_{n-1} data appears at the output of the A/D converter and the summer, the TI_{n-1} and SO_{n-1} values are read (step 220). Similarly, once the effect of the TO_n data appears at the output of the A/D converter and the summer, the TI_n and the SO_n values are read (step 224). The steps of first waiting and then reading the TI and SO values described herein can be implemented either sequentially or in parallel.

The index to the LUT which determines which coefficient is presently under calculation is then generated using the TI_{n-1} value read during step 220 (step 225). This index is used for the calibration process only and does not effect the main real time data path of the system. In the example noise reduction system shown in Figure 4, the LUT has less entries in it than the number of possible input values, e.g., 256 regions for 12 bits of input data, in order

to reduce the size of the lookup table required. Alternatively, the LUT can be constructed to hold a coefficient value for each and every possible input data.

Once the TI and SO data have been read, the new coefficients are calculated using the following equation (step 226).

$$C_{new} = C_{old} + K \left\{ \left[\frac{TO_n - TO_{n-1}}{(TI_n - SO_n) - (TI_{n-1} - SO_{n-1})} \right] - C_{old} \right\}$$

The new coefficient C_{new} is a function of the old coefficient C_{old} . The values TO, TI and SO are used to generate an intermediate new coefficient from which C_{old} is subtracted. A portion of the delta is added to C_{old} to perform the calibration. The constant K varies between 0 and 1 and is used to determine the speed with which the coefficients are permitted to change.

Values of K closer to 0 cause the coefficients to change more slowly whereas values of K closer to 1 cause the coefficients to change more quickly.

The second calibration method associated with the first noise reduction embodiment of Figure 4 will now be described in more detail. A high level flow diagram illustrating the second calibration method associated with the first embodiment is shown in Figure 9. This second method of calibration is similar to that of the first method described in connection with Figure 8, with the difference being that rather than wait for the actual noise source to cause a change to the TO value, an artificial noise signal is injected into the data path to simulate a known change in the noise signal level. The second method of coefficient calibration models the noise as a pseudo DC level noise source during calibration. This is a reasonable assumption since the calibration period of approximately 10 μ s is very short relative to the noise frequency. This pseudo DC level of the noise is used to point to a particular region in the linearity LUT.

With reference to Figures 4 and 9, the first step is to measure the Table Input (TI) value denoted TI_{n-1} at the output of the A/D converter 92 (step 230). The index to the linearity LUT is then generated based on the TI_{n-1} value just measured (step 232). The index determines which of the coefficients of the linearity LUT is to be calibrated during this particular invocation of the method. The next step is to read the Table Output (TO) value, denoted TO_{n-1} , at the output of the multiplier 93 and the Summer Output (SO) value, denoted SO_{n-1} , at the output of the summer 94 (step 234). The TO value is generated by multiplying the output of the A/D converter with the output of the LUT. The result of the multiplication is added to the output of the digital filter. Note that the TO and SO values are read

immediately after the TI value is read without waiting a system time delay as in the first method of Figure 8.

A calibration signal is then injected at the output of the multiplier (step 236). The output of the multiplier which is denoted as the TO value; is replaced with the calibration signal for a finite time period. The calibration signal, termed TO_n , comprises the original output of the multiplier TO_{n-1} increased by a known delta amount. The system then waits one system delay time for the injected calibration signal to appear at the output of the A/D converter (step 238). After waiting one system time delay, the data at the output of the A/D converter is read and termed TI_n . In addition, the output of the summer 94, termed SO_n , is also read (step 240).

After reading the TI_n value, the original output of the multiplier TO_{n-1} before the calibration signal was injected is restored (step 242). Then, based on the values TI, TO and SO, the new coefficient can be calculated utilizing the following equation (step 244).

$$C_{new} = C_{old} + K \left\{ \left[\frac{TO_n - TO_{n-1}}{(TI_n - SO_n) - (TI_{n-1} - SO_{n-1})} \right] - C_{old} \right\}$$

The new coefficient C_{new} is a function of the old coefficient C_{old} . The values TO, TI and SO are used to generate an intermediate new coefficient from which C_{old} is subtracted. A portion of the delta is added to C_{old} to perform the calibration. The constant K varies between 0 and 1 and is used to determine the speed with which the coefficients are permitted to change. Values of K closer to 0 cause the coefficients to change more slowly whereas values of K closer to 1 cause the coefficients to change more quickly. Further, if it is assumed that within the relatively short calibration time, the noise source changes very little, i.e. SO_n is equal to SO_{n-1} in the equation above, these terms may be removed from the equation.

The second embodiment of the noise reduction system of the present invention will now be described in more detail. A high level block diagram of a second embodiment of the noise reduction system of the present invention utilizing a computational method to reduce echoes and oscillations is shown in Figure 10. The noise reduction system of Figure 10, generally referenced 170, is constructed similarly to the noise reduction system 80 of Figure 4. The difference being the system 170 does not include the echo canceler circuit 95. The system 170 comprises an input transducer 172 such as a microphone, anti aliasing filter 174, fixed gain amplifier 176, A/D converter 178 and digital low pass filter 180.

The output of the low pass filter is corrected for non linearities of the transducers via a non linearity correction circuit comprising multiplier 186, sigma generator 183, coefficient processor 182 and linearity look up table (LUT) 184.

The output of the multiplier is input to an input decoder 188 which functions to
5 remove feedback picked up by the input transducer that was output by the output actuator. The output of the input decoder is amplified via a variable gain amplifier 192 whose gain is set by a gain control circuit 190. The output of the variable gain amplifier is input to the delayed cancellation circuit 194 whose output is added to the amplified signal via summer 196. The output of the summer is input to a D/A converter 197. The output of the D/A
10 converter is input to a low pass filter (LPF) 198. The output of the LPF is input to a power amplifier 200 whose output drives the output actuator 202 which may comprise a low delay loudspeaker.

Like components of the noise reduction system of Figure 10 function similarly to the corresponding components of the noise reduction system of Figure 4 and are thus described in
15 more detail hereinabove. Note also that a hybrid I/O device can be used with the system 170 in place of a separate input transducer and output actuators.

The goal of the noise reduction system of Figure 10, as with the system of Figure 4 also, is to detect the relatively low noise signal from the larger signal picked up from the output of the loudspeakers. The performance of the system of Figure 10 is slightly less than
20 the performance of the system of Figure 4 due to the fact that the echo canceler 95 functions to cancel acoustic echoes. The input decoder 188 functions to remove the effect of the feedback from the output actuators. Thus, the output of the decoder is substantially the noise signal with the output signal removed. This substantially pure noise signal is then inverted and amplified and output to the power amplifiers which drive the output actuators. As in the
25 system of Figure 4, the delayed cancellation circuit functions to remove feedback that appears a system time delay later. Decoding of the input in the presence of a first or a second delayed cancellation signal that was fed back to the input requires that the delayed output be subtracted from each input signal sample. In addition, calculation of the linearity table in the presence of a first or a second delayed cancellation signal also requires that the delayed
30 output be subtracted from each input signal sample.

Another difference from the system of Figure 4 is that the digital data is output from the digital low pass filter 180 to the input decoder 188 via the multiplier 186. The input

decoder 188 functions to discern the interference noise signal from the input signal which includes a feedback signal having a relatively large amplitude. The input decoder comprises a Σ generator similar to the Σ generator 183 of the non linearity correction circuit and which is described in more detail below with reference to the flow diagram of Figure 12. . Note that
5 the high level flow diagrams describing the method of linearity table calibration describe the calibration of a single coefficient. These method are repeated in order to calibrate all the coefficients.

A high level flow diagram illustrating the first calibration method associated with the second embodiment is shown in Figure 11. The first method of calibration utilizes the fact
10 that the noise is physical and continuous. The controller in the system tracks the relationship between values termed Table Input (TI), Table Output (TO) and sigma (Σ) during operation of the system. The TI values are measured at the input to the LUT 184. The TO values are measured at the output of the multiplier 186. The Σ values are generated by the Σ generator 183. The coefficient processor functions to calculate new LUT coefficients based on the TI,
15 TO and Σ values.

The calibration of the LUT coefficients during operation of the system attempts to ignore the effects of the noise source. Note that the input noise source itself changes between two adjacent samples.. The calibration method measures two adjacent TO values at the output of the multiplier 93 (Figure 10). Subsequently, the controller then measures two
20 adjacent TI values that are based on the previously measured TO values, assuming the system delay is known. The signal fed back from the output actuator to the input transducer is removed from the TI value to yield an input value that reflects the noise level only. Subsequently, the effect of the noise source is removed from the TI value.

To aid in understanding the calibration method described herein, the method of
25 removing feedback signals from the input signal implemented by the Σ generator 183 will first be described in more detail. A high level flow diagram illustrating the echo removal method of the present invention utilized in the second embodiment of the noise reduction system is shown in Figure 12. It is assumed that the initial speaker output is equal to zero and that the initial Σ is equal to zero. The first step is to sample the input value and set Σ to be
30 equal to the input value in order to drive the output actuator 202 (Figure 10) (step 270). Next, the system waits for the effect of the output value to appear at the output of the LPF 180 , i.e., the Table Input (TI) value, (step 272). The time needed for the output to propagate round trip

is termed the system delay time. The system delay time must be known and is typically measured at the time the system is installed after it is first powered on.

Once the effect of the output value appears at the TI, the input value is read and denoted TI_{n-1} (274). This input value, however, reflects both the noise level and the output that was fed back through the input. The system then starts examining input samples in order to detect a change in the input value. When a change is detected, a second input value is read and denoted TI_n (step 276). The delta Δ between the two input values is then calculated and added to a running sum Σ (step 278). The Σ value is then amplified in order to drive the actuator (step 280). The sum is initialized to zero at system startup time and is updated for each change in the input value. The running sum can be expressed as the following.

$$\Delta = TI_n - TI_{n-1}$$
$$\Sigma = \Sigma + \Delta$$

These calculations are performed each time there is a change in TI except during the period within a system delay and one clock period after system delay, as shown in the Table 1 below. As an alternative, the above calculations may be performed once every system clock except during the period that is during the system delay and one clock after system delay, as shown in Table 1 below, regardless of the resulting value of Δ . Note that the value of Δ may often be zero due to the slowly varying input signal relative to the sampling frequency of the A/D converter.

Note that the resolution of the A/D converter 178 (Figure 10) is chosen to correspond to the input changing every 10 μ s. The following table is presented to illustrate the method of Figure 12.

Table 1

System Operation Period	1	2	3	4	5	6	7	8	10 μ s delay	9	10	10 μ s delay	11
Noise Input	1	1	1	1	2	2	2	3		3	2		2
Total Measured Input (TI)	1 (TI ₁)	11 (TI ₂)	11 (TI ₃)	11 (TI ₄)	12 (TI ₅)	22 (TI ₆)	22 (TI ₇)	23 (TI ₈)		33 (TI ₉)	32 (TI ₁₀)		32 (TI ₁₁)
Δ	none							1			-1		
Σ	1	1	1	1	2	2	2	3	2	3	2	2	2
Speaker Output Reflected to the Input	0	10	10	10	10	20	20	20		30	30		20
Δ Calculation	X	X			TI ₅ -TI ₂	X		TI ₈ -TI ₆		X	TI ₁₀ -T I ₉		X
Detect Change in Input Value					*			*			*		

The following notes will aid in understanding the contents of Table 1 presented above.

1. Note that in system operation period 1 TI_{n-1} has no value, thus according to the equation given above, Δ and Σ are not defined. In this case, Σ is set equal to the input value.
2. The 'X' in the Δ calculations row means that no Δ calculations are performed in that particular system operation period.
3. The time difference between system operation periods that are not marked with '10 μ s delay' is time between samples taken by the A/D converter 178 (Figure 10). Note that there may be numerous periods between '10 μ s delay' periods, i.e., numerous periods until the noise input value changes.
4. Since the system functions to accumulate errors in measurement accuracy, the Σ accumulator does not accumulate continuously. Periodically, before the error increases above a predetermined value, the system waits until Σ becomes nearly zero at which time it sets the Σ generator to the initial conditions. Thus, regardless of the history, the system starts over from period 1 as shown in Table 1.
5. The contents of Table 1 above are associated with the operations of the Σ generator 183 and the input decoder 188 (Figure 10). It is preferable to set the operation of the two generators to the initial state as explained in Note 4 at the substantially the same time.

The total measured input is the sum of the noise input and the speaker output. The Δ and Σ values are calculated as given above and the speaker output represents the value output by the output actuator as sensed in the input. In this example, the system is considered to have a gain of 10, thus the speaker output, as fed back to the input, is taken as 10 times the value of Σ . As can be seen from Table 1 above, the method effectively removes the effect of the speaker output from the input data.

With reference to Figures 10 and 11, the first step in the calibration method is to read a Table Output (TO) value at the output of the multiplier 182, termed TO_{n-1} (step 300). After reading the TO_{n-1} value, the system waits for the difference between TO_{n-1} and TO_n at the output of the multiplier to reach a predetermined minimum before reading the next TO value which is termed TO_n (step 302). This minimum determines the accuracy of the coefficient calibration.

It is then determined whether TO_n is within the same region of the LUT as TO_{n-1} (step 304). This is checked in order to prevent two TO values being associated with different regions of the LUT. The calibration method calculates new coefficients for a single region of the LUT at a time. The calculations, thus, cannot span borders between regions.

Next, the system waits for the effect of the TO_{n-1} value (step 306) and TO_n value (step 310) to appear at the output of the LPF. The data output by the LPF is termed Table Input (TI) data. Once the effect of the TO_{n-1} data appears at the output of the LPF, the TI_{n-1} value is read along with the value of the noise denoted N_{n-1} (step 308). N is the net noise extracted from the echo removal method described hereinabove and is equal to the Σ at that particular point in time. Similarly, once the effect of the TO_n data appears at the output of the LPF, the TI_n value is read along with the value of the noise denoted N_n (step 312). The steps of first waiting and then reading the TI values described above can be implemented either sequentially or in parallel.

The TI_{n-1} value is then used to generate an index into the LUT (step 314). The LUT has less entries in it than the number of possible input values, e.g., 256 regions for 12 bits of input data in order to reduce the size of the LUT. Alternatively, the LUT can be constructed to hold a coefficient value for each and every possible input data.

Once the TI and N data have been read, the new coefficient is calculated using the following equation.

$$C_{new} = C_{old} + K \left\{ \left[\frac{TO_n - TO_{n-1}}{(TI_n - \Sigma_n) - (TI_{n-1} - \Sigma_{n-1})} \right] - C_{old} \right\}$$

The new coefficient C_{new} is a function of the old coefficient C_{old} . The values TO, TI and Σ are used to generate an intermediate new coefficient from which the old coefficient C_{old} is subtracted. A portion of the delta (determined by the constant K) is added to C_{old} to perform the calibration. The constant K varies between 0 and 1 and is used to determine the speed with which the coefficients are permitted to change. Values of K closer to 0 cause the coefficients to change more slowly whereas values of K closer to 1 cause the coefficients to change more quickly.

The second calibration method associated with the first noise reduction embodiment of Figure 4 will now be described in more detail. A high level flow diagram illustrating the second calibration method associated with the second embodiment of the present invention is shown in Figure 13. This second method of calibration is similar to that of the first method

described in connection with Figure 11, with the difference being that rather than wait for the actual noise source to cause a change to the TO value, an artificial noise signal is injected into the data path to simulate a known change in the noise signal level. The method utilizes the output of the LPF 180 (TI values), the output of the multiplier 186 (TO values) and the output of the Σ generator 183 (Σ values) in performing the calibration calculations. The second method of coefficient calibration is performed very quickly relative to the frequency of the input noise. In addition, it is assumed that the smallest period of the input noise is small enough relative to the time delay of the system that it can be regarded as a DC level. This pseudo DC level of the noise is used to point to a particular region in the linearity LUT.

With reference to Figures 10 and 13, the first step is to measure the Table Input (TI) value denoted TI_{n-1} at the output of the LPF. The output of the Σ generator is also calculated and denoted Σ_{n-1} (step 250). The index to the linearity LUT is then generated based on the TI_{n-1} value just measured (step 252). The index determines which of the coefficients of the linearity LUT is to be calibrated during this particular invocation of the method. The next step is to read the Table Output (TO) value, denoted TO_{n-1} , at the output of the multiplier 186 (step 254). The TO value is generated by multiplying the output of the LPF with the output of the LUT. The result of the multiplication is input to the input decoder. Note that the TO value is read immediately after the TI value is read without waiting a system time delay.

A calibration signal is then injected at the output of the multiplier (step 256). The output of the multiplier which is denoted as the TO value is replaced with the calibration signal for a finite time period. The calibration signal, termed TO_n , comprises the original output of the multiplier TO_{n-1} increased by a known delta amount. The system then waits one system delay time for the injected calibration signal to appear at the output of the LPF (step 258). After waiting one system time delay, the data at the output of the LPF is read and termed TI_n . In addition, the output of the Σ generator 183 is read and termed Σ_n (step 260).

After reading the TI_n value, the original output of the multiplier TO_{n-1} before the calibration signal was injected is restored (step 262). Then, based on the values TI, TO and Σ , the new coefficient is calculated utilizing the following equation (step 264).

$$C_{new} = C_{old} + K \left\{ \left[\frac{TO_n - TO_{n-1}}{(TI_n - \Sigma_n) - (TI_{n-1} - \Sigma_{n-1})} \right] - C_{old} \right\}$$

The new coefficient C_{new} is a function of the old coefficient C_{old} . The values TO, TI and Σ are used to generate an intermediate new coefficient from which C_{old} is subtracted. A portion of

the delta is added to C_{old} to perform the calibration. The constant K varies between 0 and 1 and is used to determine the speed with which the coefficients are permitted to change. Values of K closer to 0 cause the coefficients to change more slowly whereas values of K closer to 1 cause the coefficients to change more quickly.

5 Note that since the calibration calculation for each coefficient occurs very quickly, the input noise source can be regarded as constant or a pseudo DC value at the time the TI values are measured. Thus, the Σ_{n-1} and Σ_n values will cancel and thus can be removed from the equation.

10 While the invention has been described with respect to a limited number of embodiments, it will be appreciated that many variations, modifications and other applications of the invention may be made.

What is claimed is:

1. An acoustic noise reduction system for reducing the effects of a noise source, comprising:

input transducer means for sensing the acoustic noise field generated by the noise
5 source and for generating an input signal therefrom;

output actuator means for generating an acoustic output field that is effective to
reduce the level of the acoustic noise field;

correction means for adjusting the input signal generated by said input transducer to
compensate for the non linear characteristics of said input transducer and
10 output actuator;

echo cancellation means for removing from the input signal a portion of the output of
said output actuator means fed back through said input transducer means, the
output of said echo cancellation means representing a signal corresponding to
substantially the noise source by itself;

15 antinoise means for generating an antinoise signal opposite in phase to said input
signal, said output actuator means generating said acoustic output field from
said antinoise signal; and

wherein said input transducer means is located in relatively close proximity to said
output actuator means.

20 2. An acoustic noise reduction system for reducing the effects of a noise source, comprising:

input transducer means for sensing the acoustic noise field generated by the noise
source and for generating an input signal therefrom;

output actuator means for generating an acoustic output field that is effective to
25 reduce the level of the acoustic noise field;

correction means for adjusting the input signal generated by said input transducer to
compensate for the non linear characteristics of said input transducer;

input decoding means for removing extraneous signals from said input signal so as to
generate a signal corresponding to substantially the noise source alone;

antinoise means for generating an antinoise signal opposite in phase to said input signal, said output actuator means generating said acoustic output field from said antinoise signal; and

wherein said input transducer means is located in relatively close proximity to said output actuator means.

3. The system according to claims 1 or 2, wherein said input transducer means comprises a microphone.

4. The system according to claims 1 or 2, wherein said output actuator means comprises at least one loudspeaker.

5. The system according to claim 1, wherein said correction means comprises:
storage means for storing a plurality of coefficients;
coefficient processing means for dynamically updating the values of said plurality of coefficients stored in said storage means; and
means for generating a corrected input signal from the contents of said storage means and said input signal.

6. The system according to claim 2, wherein said correction means comprises:
storage means for storing a plurality of coefficients;
sigma generating means for outputting a signal corresponding to substantially the noise source only;
coefficient processing means for dynamically updating the values of said plurality of coefficients stored in said storage means; and
means for generating a corrected input signal from the contents of said storage means and said input signal.

7. The system according to claims 5 or 6, wherein said means for generating a corrected input signal comprises a multiplier.

8. The system according to claims 5 or 6, wherein said storage means is divided into regions whereby a particular range of input signal values map to the same coefficient value.

9. The system according to claims 1 or 2, further comprising calibration means for dynamically updating said correction means in response to the input signal and the output of said correction means.

10. The system according to claim 1, wherein said echo cancellation means comprises:
5 a digital filter having a delay line with a number of taps whose total delay time is equivalent to at least a system time delay of said noise reduction system;
adaptation means for dynamically adjusting the coefficient values associated with each of the taps of said digital filter; and
summing means for adding the output of said digital filter with the output of said
10 correction means.

11. The system according to claims 1 or 2, wherein said antinoise means comprises:
a variable gain amplifier operative to generate an amplified signal 180 degrees
opposite in phase from said input signal; and
gain control means for dynamically controlling the gain of said variable gain
15 amplifier.

12. The system according to claim 11, wherein said gain control means is adapted to receive a manual input control signal from a user which determines the gain of said variable gain amplifier, said user able to vary the location of a quiet zone generated by said system by varying said input control signal.

20 13. The system according to claim 12, wherein said input control signal is generated by said user remotely from said system and transmitted to said system via wireless communication means.

14. The system according to claims 1 or 2, further comprising anti alias filter means for removing alias frequencies from said input signal.

25 15. The system according to claim 14, wherein said anti alias filter means comprises a low pass filter having a cutoff frequency sufficiently high enough so as to reject frequencies greater than the sampling rate utilized within said system.

16. The system according to claims 1 or 2, further comprising a low pass filter operative to reduce oscillations present in the system derived from feedback of the acoustic output field to said input transducer.
17. The system according to claims 1 or 2, further comprising delay cancellation means
5 for reducing the effect of echo signals caused by said antinoise means sensed by said input transducer.
18. The system according to claim 17, wherein said delay cancellation means comprises a digital filter whose output is added to the output of said antinoise means.
19. The system according to claim 17, wherein said delay cancellation means comprises a
10 plurality of delay cancellation circuits wherein each delay cancellation circuit is operative to reduce the effect of the echo caused by previous delay cancellation circuits.
20. The system according to claim 18, wherein said digital filter comprises a finite impulse response (FIR) digital filter.
21. The system according to claims 1 or 2, further comprising means for sampling the
15 acoustic noise field at a sampling rate approximately 1000 times or greater than the frequency of the noise source.
22. The system according to claims 1 or 2, wherein said system is operative to generate a controlled far field quiet zone.
23. The system according to claims 1 or 2, further comprising means for sampling a
20 particular point of the noise source having an arbitrary phase and effectively canceling noise radiated from other points of the noise source having the same phase.
24. The system according to claims 1 or 2, wherein said input transducer means comprises a single microphone, said output actuator means comprises a plurality of loudspeakers arranged so as to radiate energy over a wide angle.
25. The system according to claims 1 or 2, wherein said input transducer means comprises
25 a single microphone, said output actuator means comprises a plurality of loudspeakers

arranged in linear fashion, each loudspeaker radiating energy in the same direction so as to create a wall of silence.

26. The system according to claims 1 or 2, wherein said input transducer means and said output actuator means are implemented as a single input/output (I/O) hybrid device.

5 27. A method for reducing the effects of a noise source, comprising the steps of:
sensing the acoustic noise field generated by the noise source and generating an input
signal therefrom;
generating an acoustic output field that is effective to reduce the level of the acoustic
noise field;
10 adjusting the input signal generated by an input transducer to compensate for the non
linear characteristics of said input transducer and an output actuator;
removing from the input signal a portion of the output of the output actuator fed back
through said input transducer;
generating a signal corresponding to substantially the noise source by itself; and
15 generating an antinoise signal opposite in phase to said input signal, generating said
acoustic output field from said antinoise signal.

28. A method for reducing the effects of a noise source, comprising the steps of:
sensing the acoustic noise field generated by the noise source and for generating an
input signal therefrom;
20 generating an acoustic output field that is effective to reduce the level of the acoustic
noise field;
adjusting the input signal generated by an input transducer to compensate for the non
linear characteristics of said input transducer;
removing extraneous signals from said input signal so as to generate a signal
25 corresponding to substantially the noise source alone; and
generating an antinoise signal opposite in phase to said input signal, said output
actuator means generating said acoustic output field from said antinoise signal.

29. An acoustic noise reduction system according to any of claims 1- 26, substantially as described hereinabove.

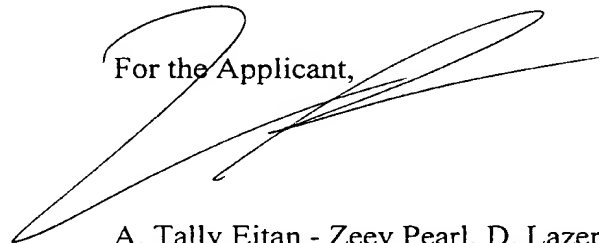
30. An acoustic noise reduction system according to any of claims 1 - 26, substantially as illustrated in any of Figures 1- 13.

31. A method of reducing the effects of a noise source according to any of claims 27- 28 substantially as described hereinabove.

5 32. A method of reducing the effects of a noise source according to any of claims 27- 28, substantially as illustrated in any of Figures 1- 13.

10

For the Applicant,

A handwritten signature in black ink, consisting of a large, stylized 'A' followed by a series of loops and a long horizontal stroke.

A. Tally Eitan - Zeev Pearl, D. Lazer & Co.

Law Offices

P-1301-IL

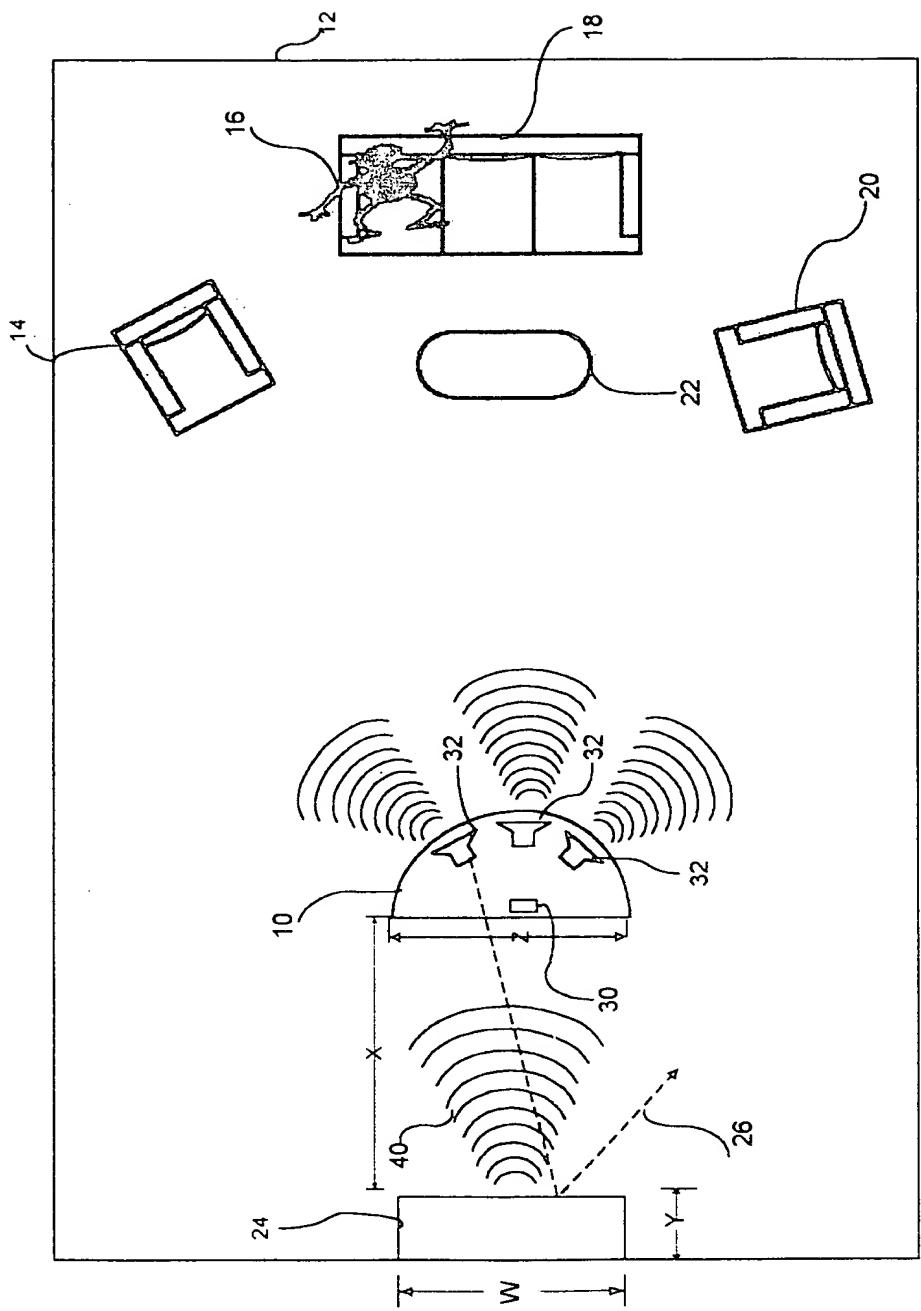
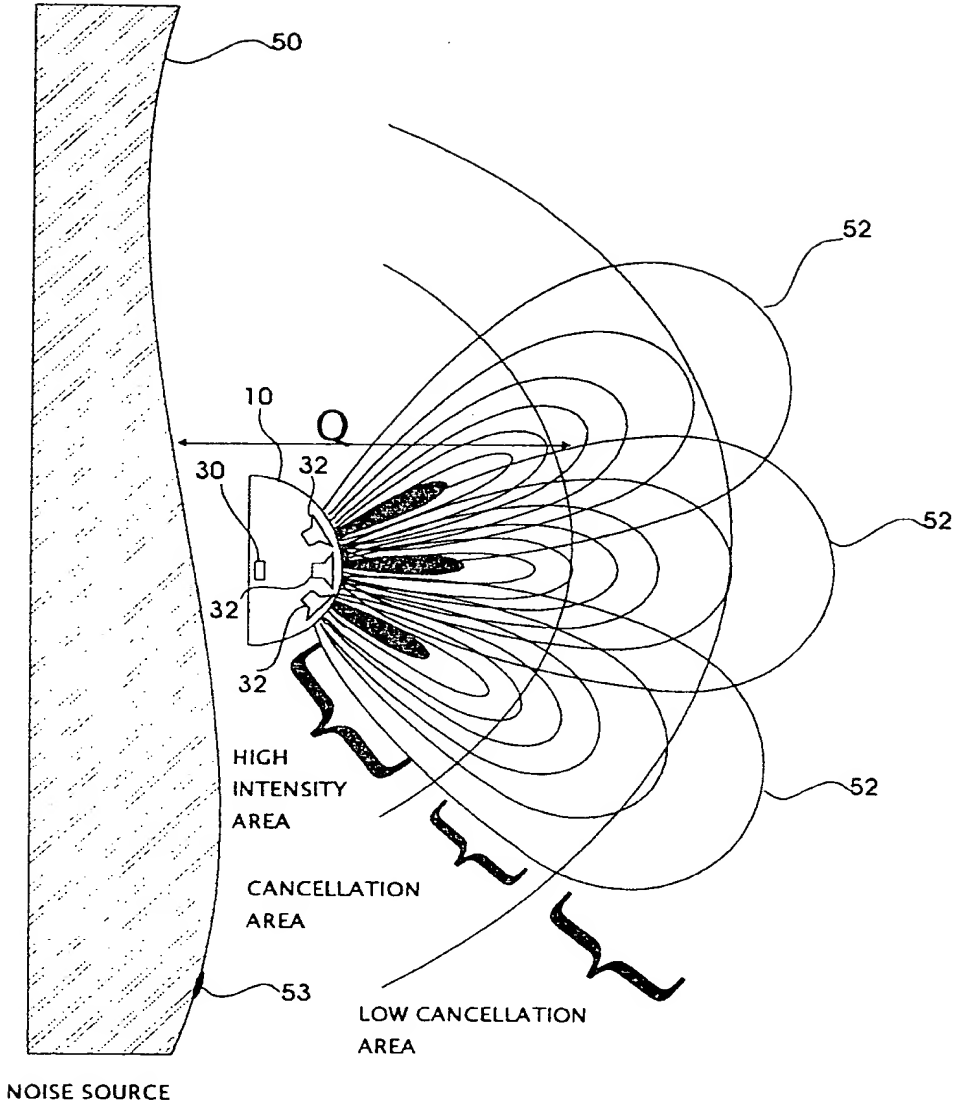


FIG. 1



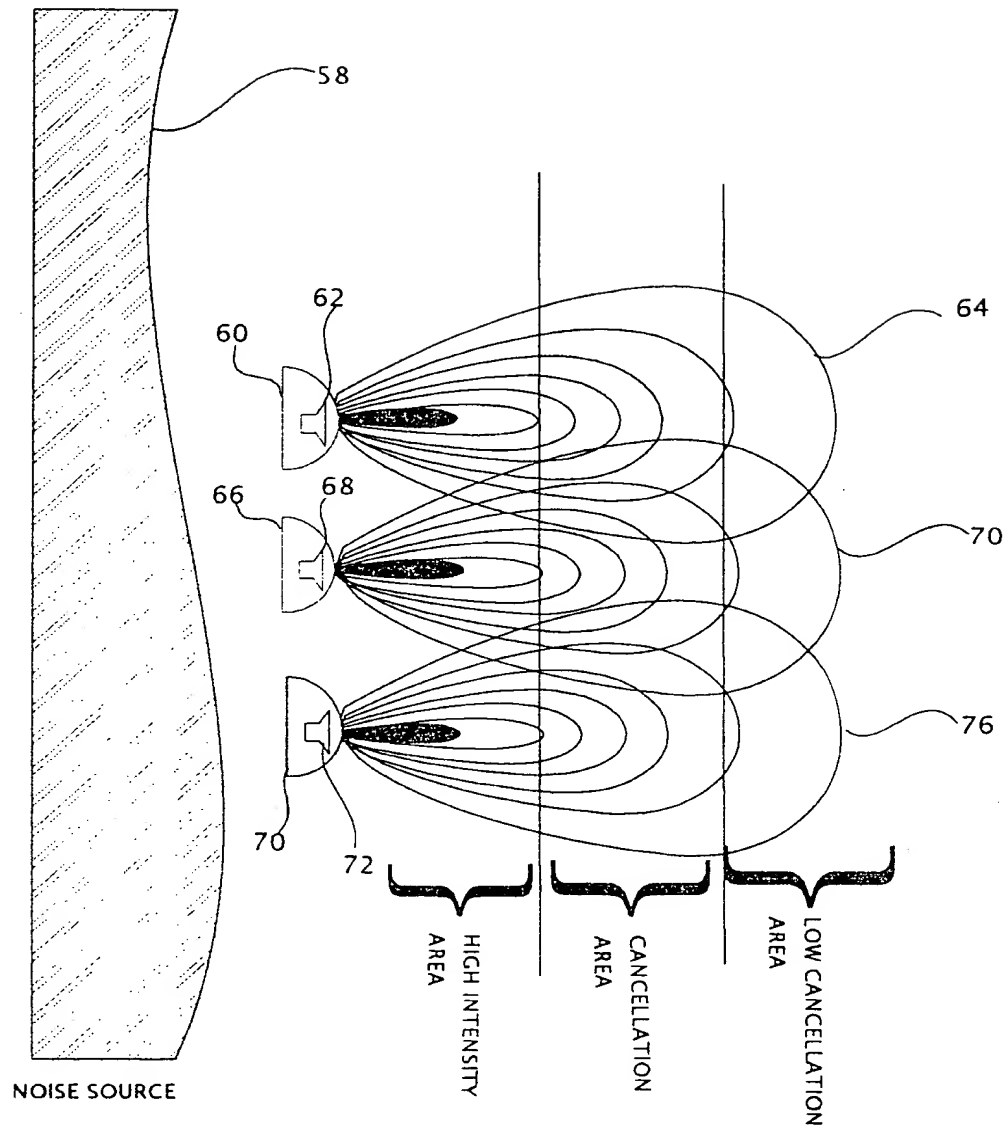


FIG. 3

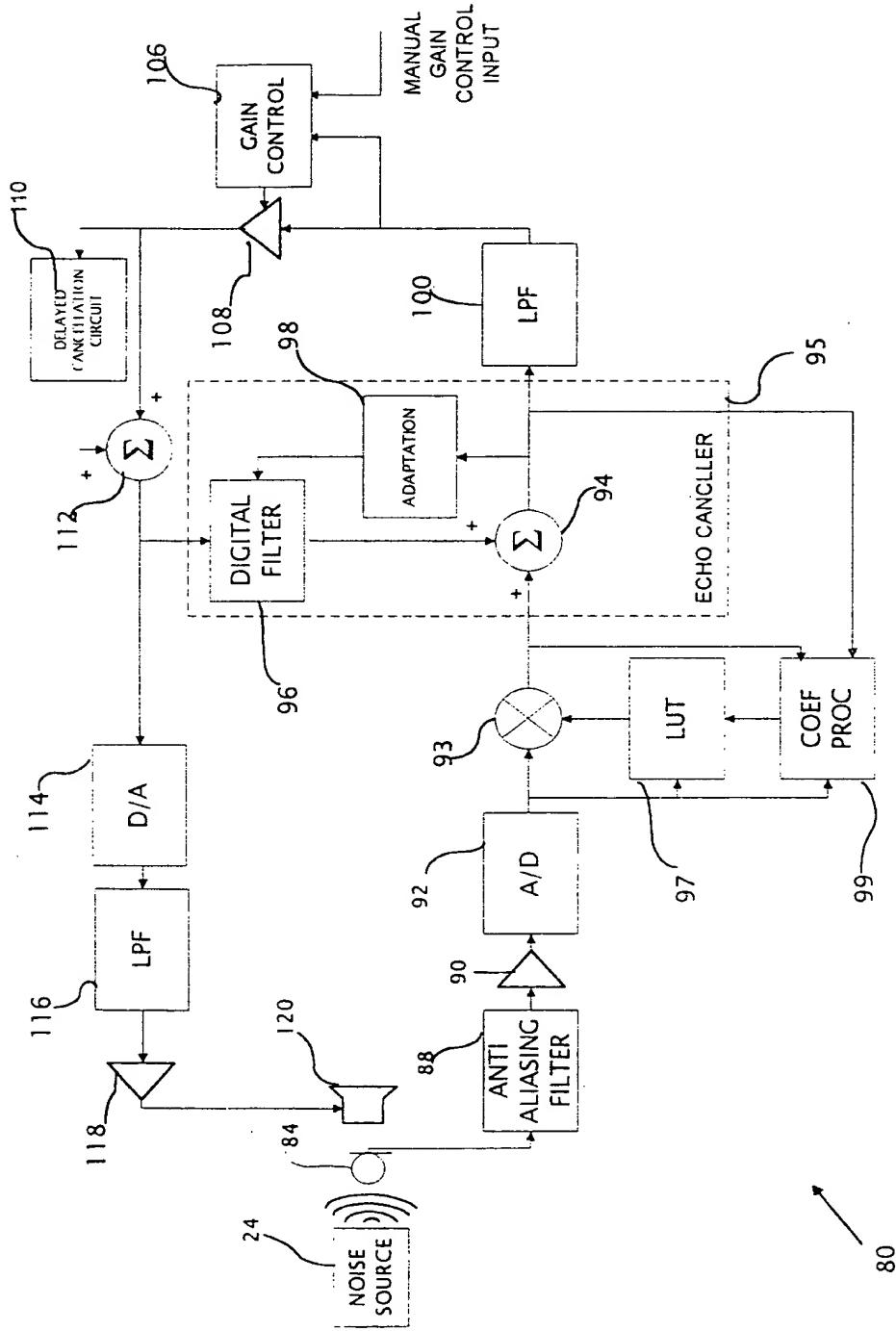


FIG. 4

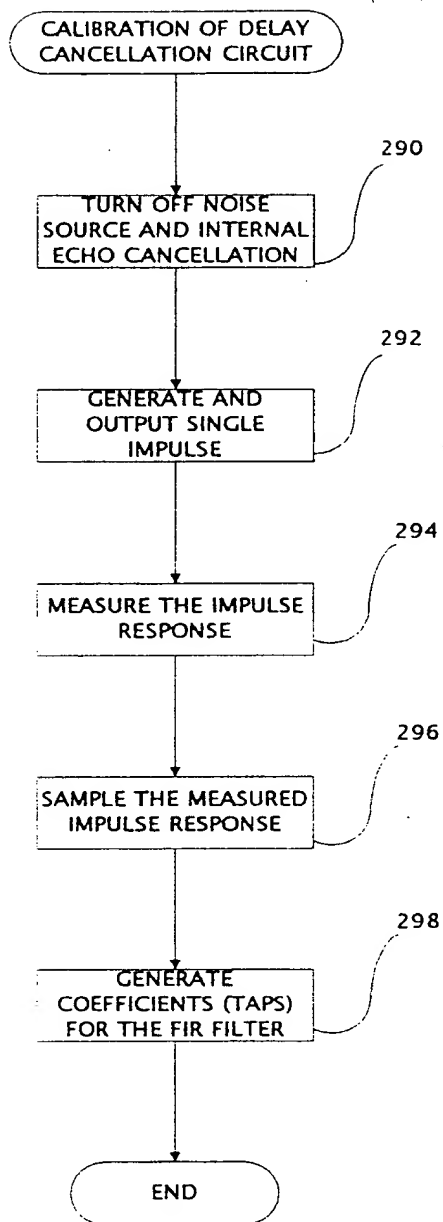


FIG. 5

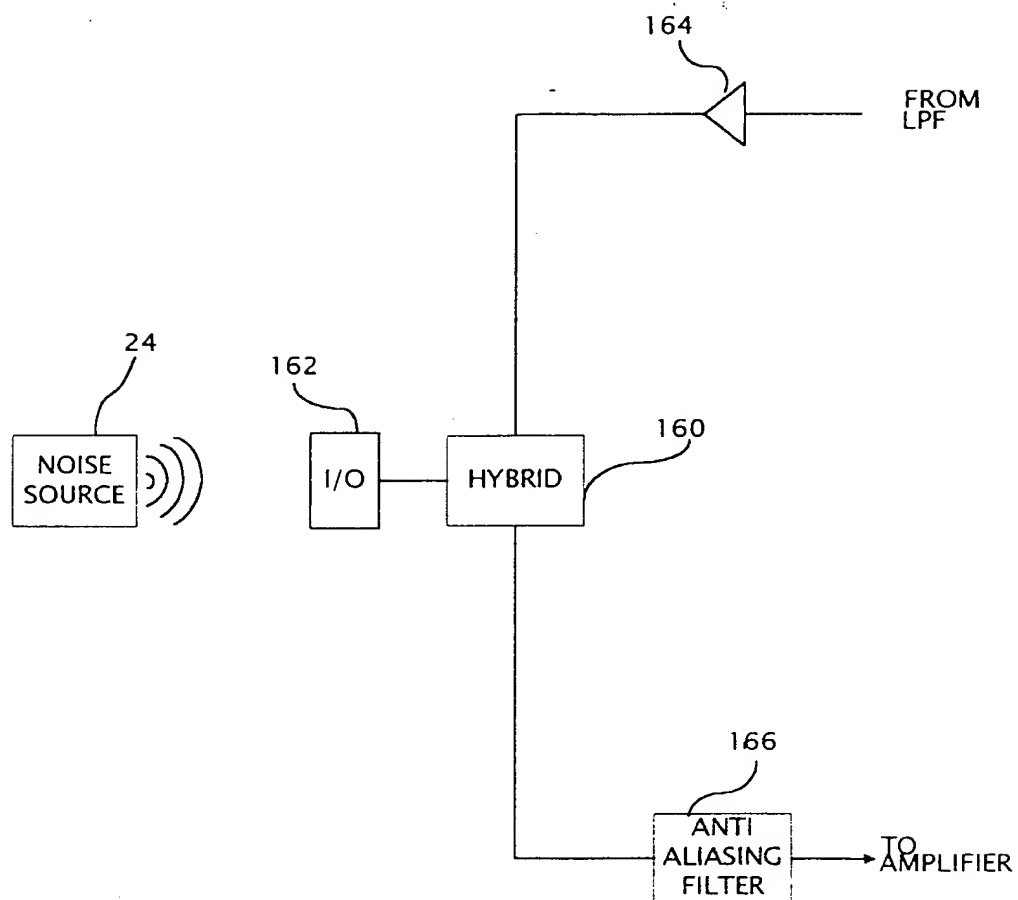


FIG. 6

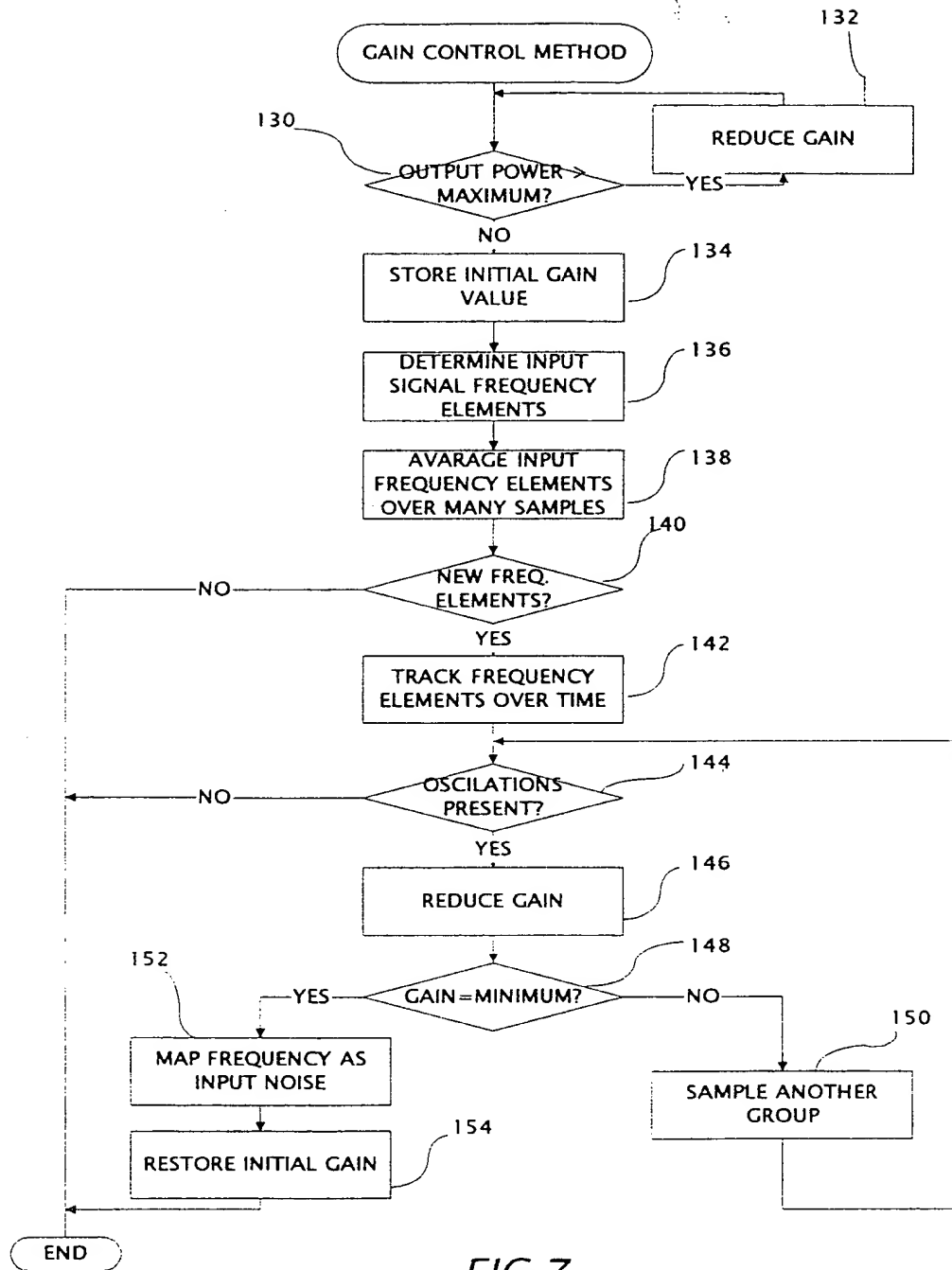


FIG. 7

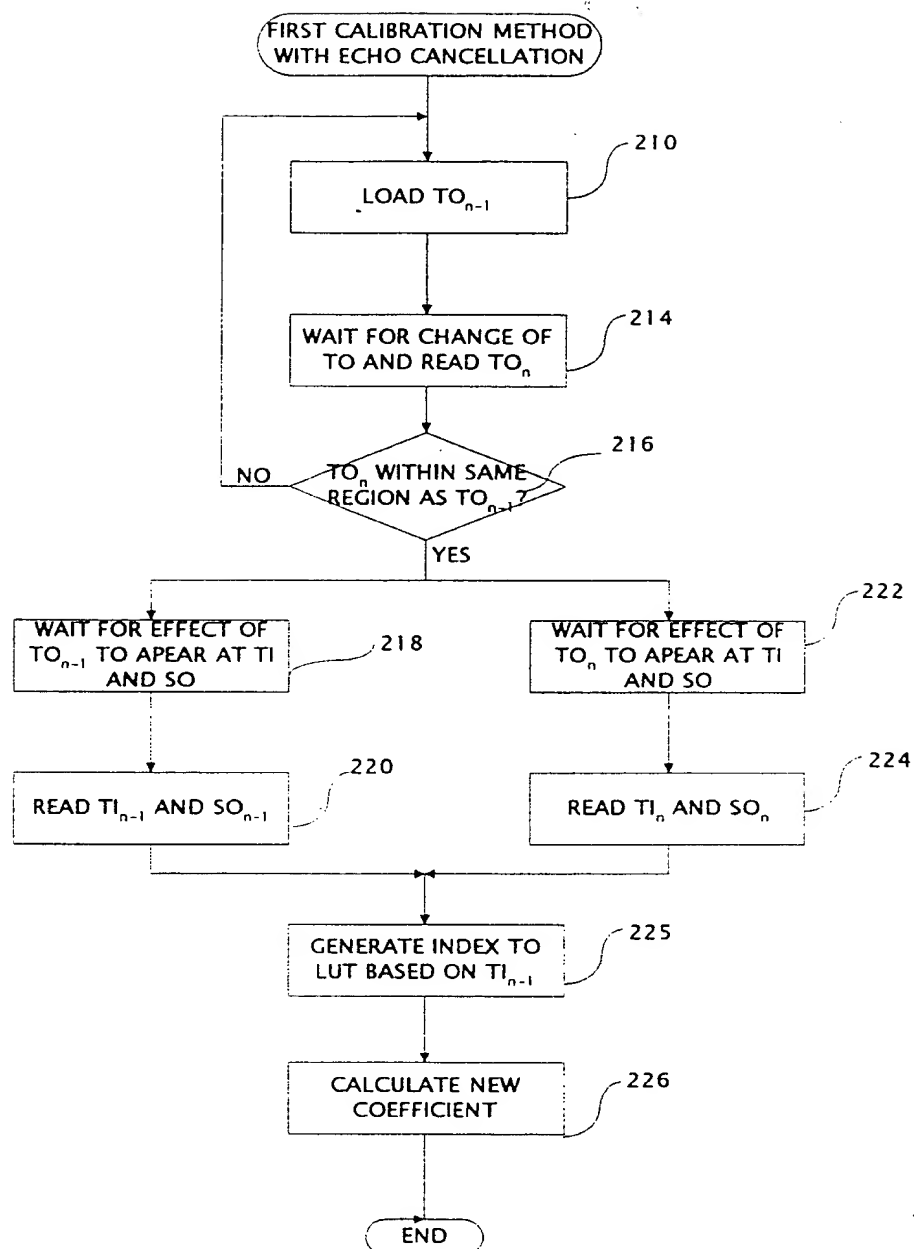


FIG. 8

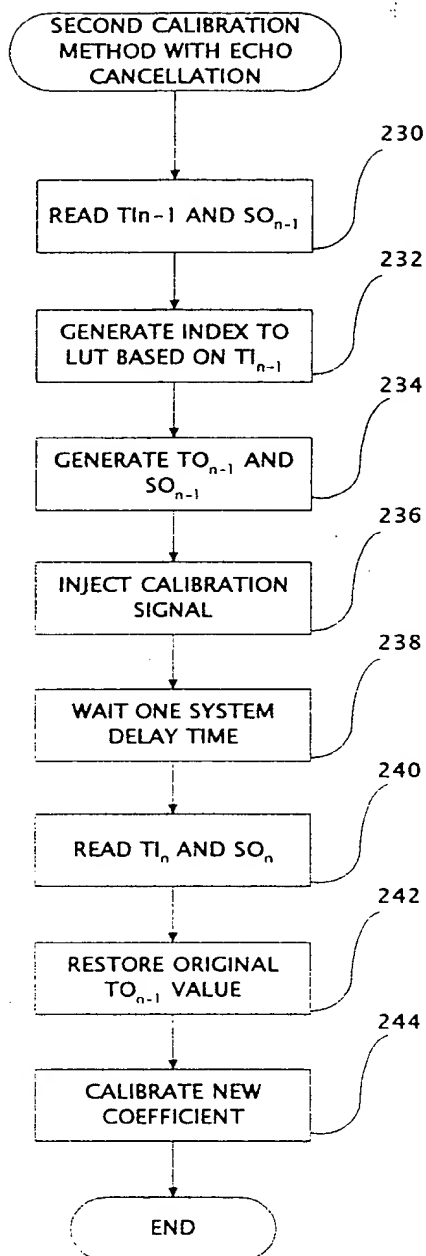


FIG. 9

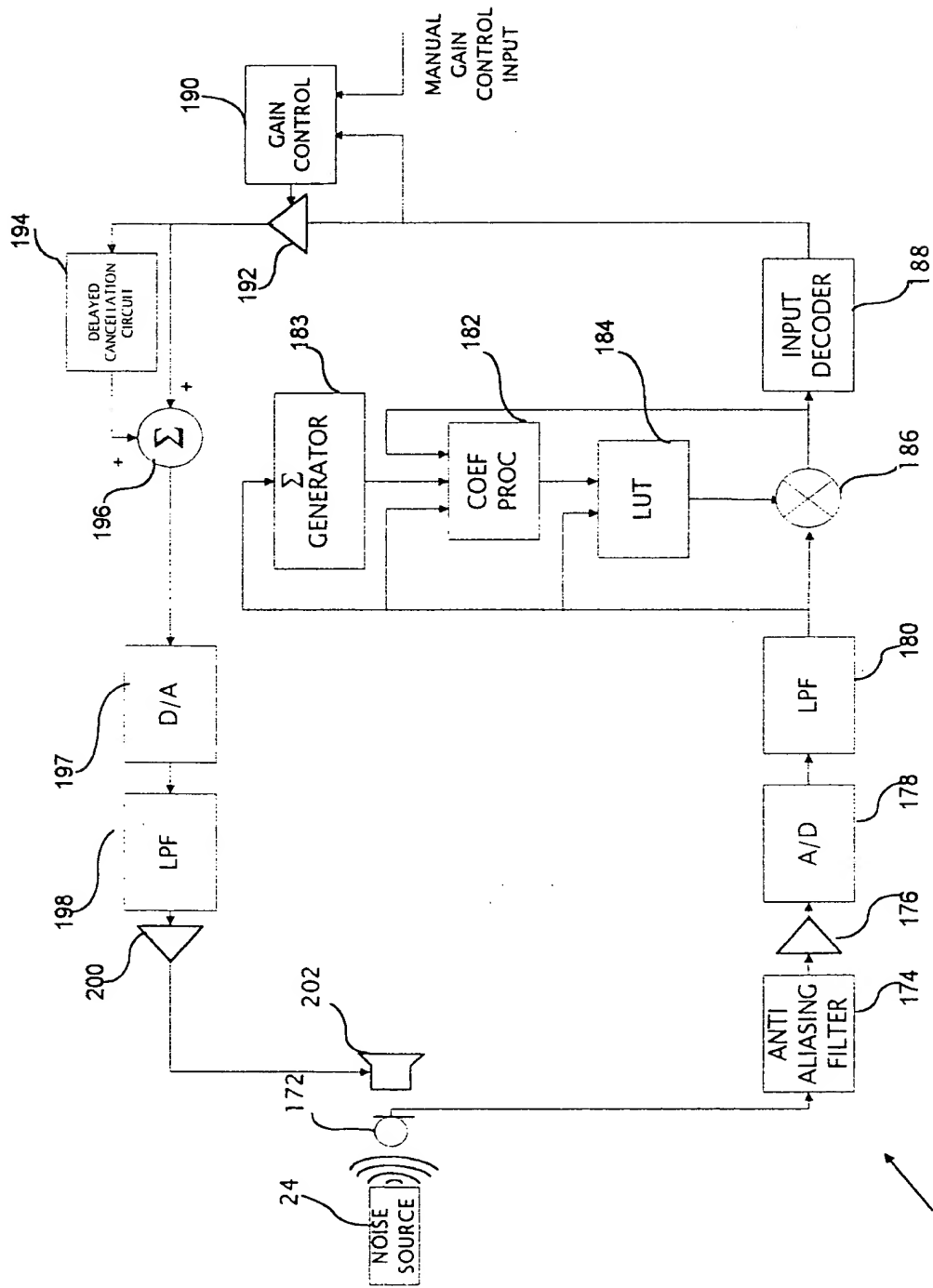


FIG. 10

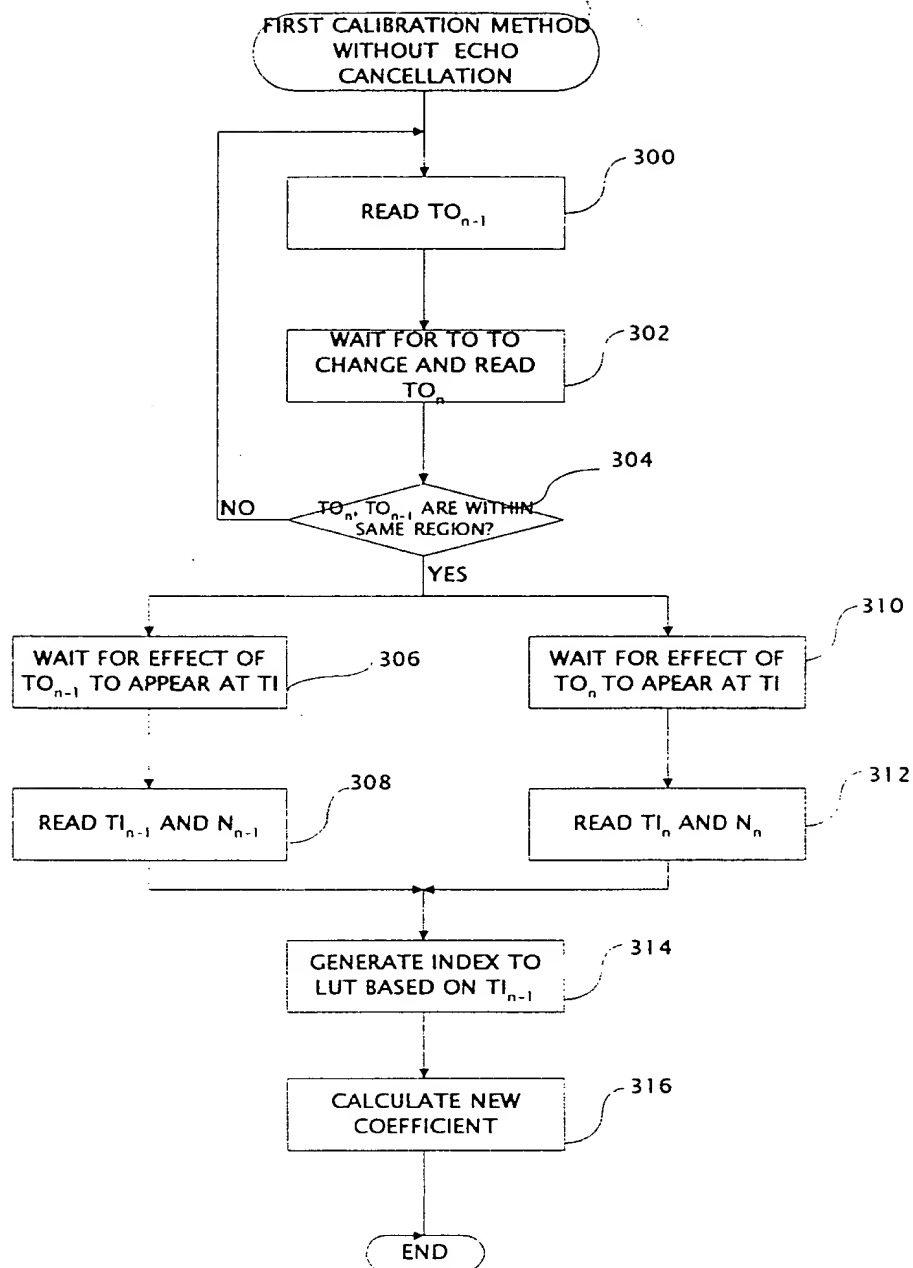


FIG. 11

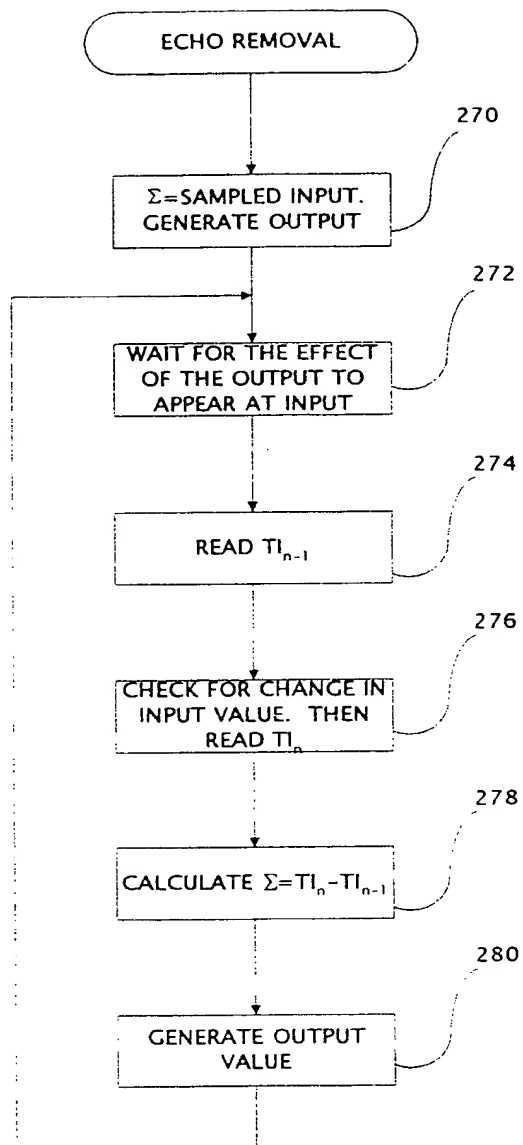


FIG. 12

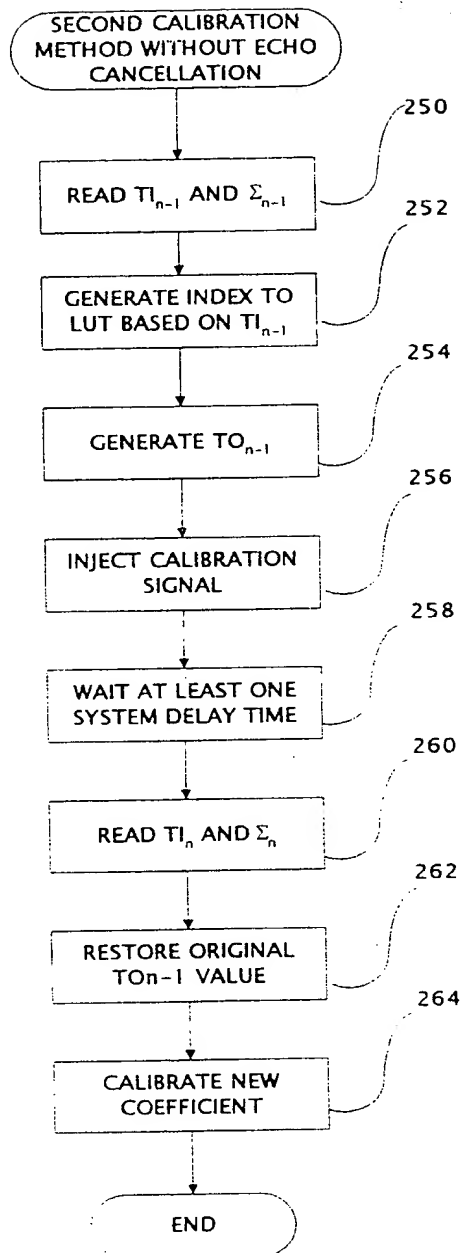


FIG. 13